

Chapter 6

Conclusion

In this dissertation an efficient and accurate quasi-static methodology is presented for evaluating frequency dependent resistance and inductance of high-speed digital interconnects and various lossy transmission lines. For circuit performance evaluation and signal integrity analysis in high-speed computer and communication systems, the prediction of parasitic resistance and inductance as well as capacitance is required especially for inter-chip interconnects, e.g., in multichip modules (MCMs), where the conductor loss becomes important as the clock speed increases. Resistance and inductance prediction is required from DC to high frequency where the skin depth is of the order of the cross-sectional dimension of the conductor. At high frequency the standard impedance boundary condition (SIBC) can be incorporated with various electromagnetic field solvers, but it is hard to apply SIBC at low and mid frequency because accurate surface impedance modeling is difficult at that regime. For unified evaluation of resistance and inductance from low to high frequency, the effective internal impedance (EII) is defined as an approximation to the surface impedance of the isolated conductor, which characterizes the interior of the conductor to represent resistance and internal inductance. Three different models of EII are presented: first, the plane wave model assumes a plane wave is incident onto all conductor surfaces and penetrates into the conductor. Second, the modified plane wave model takes care of the reflection and transmission of the plane wave inside and the interface of the conductor at low frequency and, therefore, accurately accommodates low frequency behavior. Third, the transmission line model divides the conductor into triangular patches near the corner and flat slabs, and EII is defined by solving non-uniform and

uniform telegraphist's equation. By combining the boundary element method (BEM) and EII it is demonstrated that these EII models give a good approximation to the surface impedance and are useful as SIBC at high frequency, but at low and mid frequency EII is different from SIBC.

EII should be incorporated with appropriate field solvers to accurately predict resistance and inductance, regardless of the frequency of interest. First, the conformal mapping is combined with EII, which is efficient and reasonably accurate in that it avoids numerically intensive matrix manipulation and considers the geometrical symmetry. It is applied for asymmetric transmission lines, the effect of the conductor thickness is examined, and the effectiveness is shown. But, its application to complicated multi-conductor transmission lines and three dimensional geometries is restricted due to the difficulty of finding the conformal maps. To overcome the limit of the conformal mapping technique the more rigorous, Green's function based surface current integral equation is successfully incorporated with EII for regular two dimensional transmission lines and three dimensional structures. And these are shown to be efficient and accurate through comparison with existing rigorous quasi-static techniques of the volume filament method (VFM) and the partial element equivalent circuit method (PEEC), which are based on the volume current integral equation.

The EII approach fundamentally reduces the computational time and memory by modeling the conductor interior as an impedance shell at the conductor surface and replacing the discretization of the conductor interior with the discretization of the conductor surface. Further computational efficiency can be obtainable by applying numerically fast matrix solvers such as the multipole-accelerated, preconditioned generalized minimal residual (GMRES) algorithm or other iterative solvers exploiting

sparsification of the matrix. As a next step in circuit performance evaluation of quantities such as delay, crosstalk, simultaneous switching noise, etc., the proposed technique of calculating frequency dependent resistance and inductance can be interfaced with existing convolution based or SPICE-like time domain circuit simulators, in conjunction with moment-matching methods. One way is to use frequency independent circuit representation, where the frequency dependent series impedance is approximately synthesized using lumped RL ladder circuits. The other way is to represent the impulse response of the frequency dependent lines using Y -parameters, S -parameters, etc. and, then, to simulate in the time domain by matching the nonlinear boundary conditions. In this approach the frequency dependent transmission line is modeled as a macro and it is used in a SPICE-like simulator.

Appendix

Analysis of Coupled Lossy Transmission Lines

Time domain simulation of signal propagation along lossy transmission lines is feasible with various SPICE-like or other simulators. For the circuits with linear loads, the fast Fourier transform (FFT) can be easily adopted to the analysis of the transmission lines. For coupled lossy transmission lines as shown in Fig. 4.10, the telegraphist's equation is solved with appropriate driver and load conditions as in reference [91,92] . And the following transfer functions are driven for an active and a quiet line.

$$\frac{V_{1,2}(x, \omega)}{V_{in}(\omega)} = 0.5 \left[\frac{1}{P_1} \frac{e^{-\gamma_1 x} + \rho_{L1} e^{-\gamma_1 (2l-x)}}{1 - \rho_{S1} \rho_{L1} e^{-2\gamma_1 l}} \pm \frac{1}{P_2} \frac{e^{-\gamma_2 x} + \rho_{L2} e^{-\gamma_2 (2l-x)}}{1 - \rho_{S2} \rho_{L2} e^{-2\gamma_2 l}} \right], \quad (A.1)$$

where Z_L is the load impedance, Z_S is the driver impedance, V_1 and V_2 are the voltage of an active and a quiet line, respectively.

$$\rho_{Ln} = \frac{Z_L - Z_n}{Z_L + Z_n} \quad \rho_{Sn} = \frac{Z_S - Z_n}{Z_S + Z_n} \quad P_n = 1 + \frac{Z_S}{Z_n} \quad (A.2)$$

Z_n is the characteristic impedance for even and odd mode of two lines,

$$Z_1 = \sqrt{\frac{(R_{11} + R_{12}) + j\omega(L_{11} + L_{12})}{j\omega(C_{11} - C_{12})}} \quad Z_2 = \sqrt{\frac{(R_{11} - R_{12}) + j\omega(L_{11} - L_{12})}{j\omega(C_{11} + C_{12})}} \quad (A.3)$$

and γ_n is the propagation constant for even and odd mode of two lines.

$$\gamma_1 = \sqrt{\{(R_{11} + R_{12}) + j\omega(L_{11} + L_{12})\}j\omega(C_{11} - C_{12})} \quad (A.4)$$

$$\gamma_2 = \sqrt{\{(R_{11} - R_{12}) + j\omega(L_{11} - L_{12})\}j\omega(C_{11} + C_{12})}.$$

And through a fast Fourier transform (FFT) time domain signal profile is obtained.

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